

(19) World Intellectual Property Organization
International Bureau



(43) International Publication Date
30 November 2000 (30.11.2000)

PCT

(10) International Publication Number
WO 00/72464 A1

(51) International Patent Classification⁷:
H04L 5/12, 1/16

Nokia Research Center, Itämerenkatu 11-13, FIN-00045
Nokia Group (FI).

(21) International Application Number: PCT/EP99/03440

(74) Agents: PELLMANN, Hans-Bernd et al.; Tiedtke-Büh-
ling-Kinne, Bavariaring 4, D-80336 München (DE).

(22) International Filing Date: 19 May 1999 (19.05.1999)

(25) Filing Language: English

(26) Publication Language: English

(71) Applicant (for all designated States except US): NOKIA
NETWORKS OY [FI/FI]; Keilalahdentie 4, FIN-02150
Espoo (FI).

(81) Designated States (national): AE, AL, AM, AT, AU, AZ,
BA, BB, BG, BR, BY, CA, CH, CN, CU, CZ, DE, DK, EE,
ES, FI, GB, GD, GE, GH, GM, HR, HU, ID, IL, IN, IS, JP,
KE, KG, KP, KR, KZ, LC, LK, LR, LS, LT, LU, LV, MD,
MG, MK, MN, MW, MX, NO, NZ, PL, PT, RO, RU, SD,
SE, SG, SI, SK, SL, TJ, TM, TR, TT, UA, UG, US, UZ,
VN, YU, ZA, ZW.

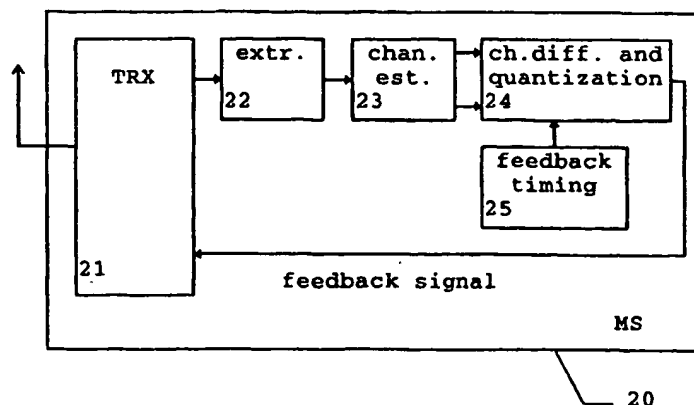
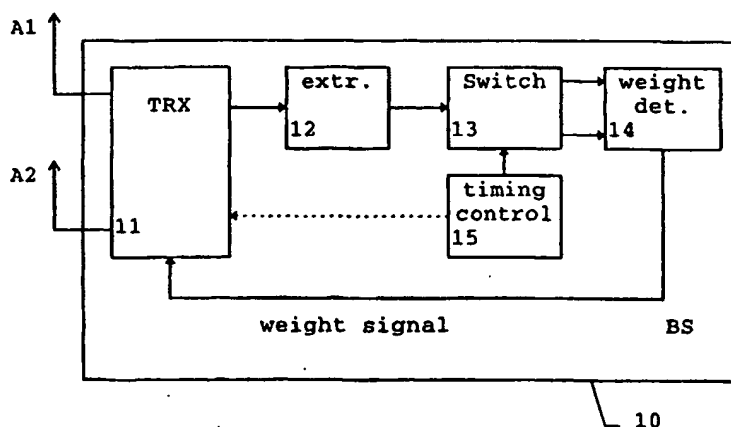
(72) Inventors; and

(75) Inventors/Applicants (for US only): HOTTINEN, Ari
[FI/FI]; Nokia Research Center, Itämerenkatu 11-13,
FIN-00045 Nokia Group (FI). WICHMAN, Risto [FI/FI];

(84) Designated States (regional): ARIPO patent (GH, GM,
KE, LS, MW, SD, SL, SZ, UG, ZW), Eurasian patent (AM,
AZ, BY, KG, KZ, MD, RU, TJ, TM), European patent (AT,
BE, CH, CY, DE, DK, ES, FI, FR, GB, GR, IE, IT, LU, MC,
NL, PT, SE), OAPI patent (BF, BJ, CF, CG, CI, CM, GA,
GN, GW, ML, MR, NE, SN, TD, TG).

[Continued on next page]

(54) Title: TRANSMIT DIVERSITY METHOD AND SYSTEM



(57) Abstract: The invention relates to a transmit diversity method for a wireless communication system comprising a transmitting element and at least one receiver, wherein a transmission signal is transmitted from the transmitting element to the at least one receiver in accordance with a weight information determined in response to a feedback information. The feedback information is derived from the response at the at least one receiver to the transmission signal, and is fed back using multiplexed feedback signals. Multiple feedback signal quantization constellations and/or constellation specific feedback subchannels can be used for channel probing, such that the total feedback resolution and robustness can be enhanced, while maintaining low signaling capacity of the feedback channel.

WO 00/72464 A1



Published:

— With international search report.

For two-letter codes and other abbreviations, refer to the "Guidance Notes on Codes and Abbreviations" appearing at the beginning of each regular issue of the PCT Gazette.

- 1 -

Transmit diversity method and systemFIELD OF THE INVENTION

5 The present invention relates to a transmit diversity method and system for a wireless communication system, such as the Universal Mobile Telecommunications System (UMTS) comprising a transmitting element and at least one receiver.

10

BACKGROUND OF THE INVENTION

Wideband Code Division Multiple Access (WCDMA) has been chosen as the radio technology for the paired bands of the UMTS. Consequently, WCDMA is the common radio technology standard for third-generation wide-area mobile communications. WCDMA has been designed for high-speed data services and, more particularly, Internet-based packet-data offering up to 2Mbps in indoor environments and over 384 kbps for wide-area.

The WCDMA concept is based on a new channel structure for all layers built on technologies such as packet-data channels and service multiplexing. The new concept also includes pilot symbols and a time-slotted structure which has led to the provision of adaptive antenna arrays which direct antenna beams at users to provide maximum range and minimum interference. This is also crucial when implementing wideband technology where limited radio spectrum is available.

The uplink capacity of the proposed WCDMA systems can be enhanced by various techniques including multi-antenna reception and multi-user detection or interference cancellation. Techniques that increase the downlink

- 2 -

capacity have not been developed with the same intensity. However, the capacity demand imposed by the projected data services (e.g. Internet) burdens more heavily the downlink channel. Hence, it is important to find techniques that
5 improve the capacity of the downlink channel.

Bearing in mind the strict complexity requirements of terminals, and the characteristics of the downlink channel, the provision of multiple receive antennas is not a desired
10 solution to the downlink capacity problem. Therefore, alternative solutions have been proposed suggesting that multiple antennas or transmit diversity at the base station will increase downlink capacity with only minor increase of complexity in terminal implementation.

15

According to the WCDMA system, a transmit diversity concept is under consideration which is mainly focused on the closed-loop (feedback) mode.

20 Fig. 1 shows an example of such a feedback mode for a downlink transmission between a base station (BS) 10 and a mobile terminal or mobile station (MS) 20. In particular, the BS 10 comprises two antennas A1 and A2, and the MS 20 is arranged to estimate the channel on the basis of two
25 transmission signals received from the two antennas A1 and A2. Then, the MS 20 feeds back the discretized channel estimate to the BS 10. Naturally, it is desired to develop a robust and low-delay feedback signaling concept.

30 In WCDMA, three modes are suggested for the closed-loop concept which is optimized for two antennas. In the feedback (FB) mode 1 (also referred to as Selective Transmit Diversity (STD)), one bit per time slot is used to signal the "best" antenna from each terminal. The remaining
35 closed-loop FB modes 2 and 3 provide a slower feedback

- 3 -

link, where feedback weights used for controlling the antennas A1 and A2 are modified after two or four 0.625 ms slots, respectively. In this case, the antennas A1 and A2 are co-phased so that transmitted signals sum up coherently in the MS 20, to thereby provide the best performance with low mobility "low multipath" environments.

Fig. 2 shows a table indicating characteristic parameters of the above FB modes 1 to 3. In particular, N_{FB} designates the number of feedback bits per time slot, N_W the number of bits per feedback signaling word, N_a the number of feedback bits for controlling an amplification or power at the antennas A1 and A2, and N_p the number of feedback bits for controlling a phase difference between the antennas A1 and A2. As can be gathered from the table of Fig. 2, one bit is fed back per time slot in each of the FB modes 1 to 3.

In the FB mode 1 (i.e. STD), the bit length of the feedback signaling word is one bit, which leads to an update rate of 1600/s (i.e. an update is performed at the BS 10 in every time slot). The feedback bit rate is 1600 bps and the feedback signaling word is used for controlling the power supplied to the antennas A1 and A2.

In the FB mode 2, the feedback signaling word comprises two bits, which leads to an update rate of 800/s, since an update is performed after both feedback bits have been received, i.e. after two time slots. The feedback signaling word is only used for controlling the phase difference between the two antennas A1 and A2.

In the FB mode 3, the bit length of the feedback signaling word is four, such that an update rate of 400/s is obtained, i.e. an update is performed every four time slots. In particular, one bit of the feedback signaling

- 4 -

word is used for controlling the amplification (power) at the antennas A1 and A2, and three bits are used for controlling their phase difference.

5 Fig. 3A shows a table indicating the feedback power control performed in the FB mode 1 or STD. Here, the MS 20 has to estimate the antenna with the smallest path loss. To this effect, the MS 20 estimates the channel power of all "competing antennas", and determines the one with the
10 highest power. The required channel estimates are obtained e.g. from a common pilot channel transmitted with a known power from each antenna. The table in Fig. 3A shows the relationship between the feedback value and the power P_{A1} supplied to the antenna A1 and the power P_{A2} supplied to
15 the antenna A2. Accordingly, one of the two antennas A1 and A2 is selected at the BS 10 in response to the feedback signaling value.

It is to be noted that the FB mode 1 may be implemented in
20 an analog manner in the beam domain. In this case, the MS 20 signals to the BS 10 whether to rotate channel symbols transmitted from the antenna A2 by 180° . In this case, the BS 10 transmits simultaneously from both antennas A1 and A2. Thus, the phase difference between the antennas A1 and
25 A2 is switched between 0° and 180° in response to the feedback value.

The other FB modes 2 and 3 relate to a feedback concept referred to as Transmission Antenna Array (TxAA), in which
30 the MS 20 transmits estimated and quantized channel parameters to the BS 10 which then weights the transmitted signals accordingly.

Fig. 3B shows the feedback control performed in the FB mode
35 2. In the FB mode 2, only a phase weight feedback value

- 5 -

comprising two bits is fed back to the BS 10. The phase difference indicated in the table of Fig. 3B defines the phase difference (in degree) between the antennas A1 and A2, which is to be established by the BS 10 in order to
 5 obtain an optimum coherence at the MS 20.

Fig. 3C shows the feedback control of the FB mode 3, wherein one bit, i.e. amplification bit, of the feedback signaling word is used for controlling the power of the
 10 antennas A1 and A2, and the other three bits, i.e. phase bits, are used for controlling the phase difference between the antennas A1 and A2. The left-hand table indicates the power control based on the amplification bit, wherein the power P_{A1} and P_{A2} supplied to the antennas A1 and A2,
 15 respectively, is switched between 20% and 80% of a predetermined value. The right-hand table shows the feedback control based on the three phase bits, wherein the phase difference can be quantified into eight different phase difference values to be established by the BS 10 in
 20 order to obtain an optimum coherence in the MS 20.

As regards the table of Fig. 2, it is to be noted that an equal power is applied to the antennas A1 and A2 in each case where $N_a = 0$. Furthermore, the antennas A1 and A2 are
 25 uniquely defined by their respective pilot codes of the CCPCCH (Common Control Physical Channel) of the UMTS. The derived amplitude and phase applied to the antennas A1 and A2 is called a weight and the set of weights is grouped into a weight vector. Specifically, the weight vector for
 30 the present case of two antennas is given by

$$\underline{w} = \left[\frac{\sqrt{P_{A1}}}{\sqrt{P_{A2}} \cdot \exp(j\pi\Delta\varphi / 180)} \right]$$

- 6 -

wherein $\Delta\phi$ denotes the phase difference (phase weight) fed back to the BS 10. In case the dimension of \underline{w} becomes larger than two, more than two antennas, i.e. an antenna array, are required, wherein a directional antenna is achieved by using relative phases between antennas. The estimated phase of the feedback signal in the complex plane is then used for controlling the transmit direction.

Hence, the current WCDMA transmit diversity feedback concept uses a 2, 4 or 8 phase constellation to signal the channel difference to the BS 10. However, the higher channel resolution provided by a higher constellation order is obtained at the expense of feedback signaling capacity. Thus, the resolution of the feedback signaling is limited by the feedback signaling capacity. Furthermore, the current concept imposes a delay of one or more slots in executing the weight change and this restricts applicability only to very slow fading channels.

SUMMARY OF THE INVENTION

It is therefore an object of the present invention to provide a method and system for transmit diversity or transmit beamforming, by means of which the resolution of the feedback signaling can be increased without increasing the feedback signaling capacity.

This object is achieved by a transmit diversity method for a wireless communication system comprising a transmitting element and at least one receiver, said method comprising the steps of:

transmitting from said transmitting element to said at least one receiver a transmission signal in accordance with a weight information determined in response to a feedback information;

- 7 -

deriving said feedback information from the response at said at least one receiver to said transmission signal; feeding back said feedback information using multiplexed feedback signals.

5

Additionally, the above object is achieved by a transmit diversity system for a wireless communication system, comprising:

transmitting means for transmitting a transmission signal
10 from a transmitting element in accordance with a weight information determined in response to a feedback information; and

at least one receiver for receiving said transmission signal and deriving said feedback information from the
15 response to said transmission signal;

wherein said at least one receiver comprises a feedback means for feeding back said feedback information using multiplexed feedback signals.

20 Furthermore, the above object is achieved by a transmitter for a wireless communication system, comprising:
extracting means for extracting a feedback information from a received signal;

transmitting means for transmitting a transmission signal
25 from a transmitting element in accordance with a weight information;

determining means for determining the weight information in response to the extracted feedback information; and

control means for controlling the determining means so as
30 to determine said weight information in accordance with multiplexed feedback signals used for feeding back said feedback information.

Moreover, the above object is achieved by a receiver for a
35 wireless communication system, comprising:

- 8 -

receiving means for receiving a transmission signal;
deriving means for deriving a feedback information from the
response to said transmission signal; and
feedback means for feeding back said feedback information
5 using multiplexed feedback signals.

Accordingly, the transmit resolution can be enhanced by
maintaining the feedback channel resolution and capacity
signaled from the receiver and performing a suitable
10 feedback filtering at the transmitter in accordance with
the time-varying feedback signal constellation. Thereby,
the effective resolution of the total feedback signaling
can be improved while maintaining the signaling channel
capacity, since the feedback information can be divided and
15 spread over different sets of time slots in accordance with
the time-varying signal constellation, or by using multiple
different constellations. The filtering is applied to at
least two subchannels. The transmitting signal may comprise
a probing signal used for channel measurements and channel
20 quantization and an information transmitted via the
dedicated channel on the basis of the transmit weights.

According to the invention, multiplexed feedback signals
can be used for representing the quantized state of the
25 channel. Thereby, the type, coding, partitioning or
allocation of the feedback signals may differ in different
multiplex subchannels defined by a time division, frequency
division, or code division multiplexing scheme. -

30 Thus, the weights applied to the antennas A1 and A2 can be
demultiplexed from the feedback channel and need not be
identical with the feedback signaling of the current time
slot received from the receiver. In particular, a multiplex
timing can be arranged such that the current FB modes still
35 can be established. Each subchannel may independently

- 9 -

define a basic resolution, and the subchannels may jointly define an increased resolution. According to the invention, at least two feedback subchannels are used. The multiplexed feedback signals are demultiplexed at the transmitting
5 element and then filtered in order to obtain the desired transmit weights. Thus, a flexible feedback concept is achieved, in which the transmit weights are derived from the feedback signals but need not match them exactly.

10 Furthermore, a higher transmit weight resolution and robustness can be achieved e.g. by multiplexing different feedback signals which are to be combined in a suitable way, e.g. by a Finite Impulse Response (FIR) filtering or an Infinite Impulse Response (IIR) filtering, at the
15 transmitter. The filtering can also take into account the reliability of the received feedback signals. Then, the filter can determine the weights based on a higher weighting of the reliable feedback signals. Therefore, the present FB mode 3 can be achieved, since it can be
20 established on the basis of e.g. the present FB mode 2 by multiplexing two different feedback signals and filtering them suitably. In this case, the feedback signaling and the channel estimation can be maintained, while slightly changing the feedback signal determination. However, no
25 changes are required to the common channels.

The length of the filter impulse response should be matched to the channel characteristics (e.g. Doppler spread) in the sense that longer filters can be used when channel changes
30 are slow. The type of filter can be determined from the received signal or it can be negotiated between the transmitter and the receiver. Furthermore, the demultiplexing and subsequent filtering can be performed on the feedback signal or on the transmit weights to which the
35 feedback signals correspond, or both. In particular, gain

- 10 -

and phase information can be filtered separately or jointly. The filter can operate as a predictor, so that transmit weights can be predicted based on the available smoothed information until the command is transmitted, 5 current weights and/or previous weights and/or received feedback commands. In addition, the filtering can be linear or non-linear. Furthermore, a robust filtering, e.g. using a median filtering, can be applied, which is preferred, since feedback errors may cause "outliers" weights, i.e. 10 erroneous weights due to a wrong index rather than an estimation error in determining the index/quantization.

Hence, the channel is quantized to a plurality of feedback signal quantization constellations, and each quantized 15 value is transmitted via different multiplexed feedback subchannels. Thereby, a user may use different channel quantization constellations at different quantization intervals which may possibly overlap. The different quantization constellations may be independent, e.g. 20 suitable rotations of each other, or may be formed in a dependent or hierarchical manner by a set partitioning, wherein the dependent constellations are jointly used to define the feedback signal with increasing accuracy (e.g. the first two bits transmitted in a first subchannel may 25 designate a weight quadrant, and the third bit transmitted in a second subchannel may specify one of two weight points within the weight quadrant). Furthermore, different quantization constellations can be provided for different users.

30

Preferably, the multiplexed feedback signals may comprise a first feedback signal having a first constellation and a second feedback signal having a second constellation. The first and second feedback signals may be transmitted in 35 different time slots and/or by using different codes.

- 11 -

The first feedback signal may define a first phase weight determined on the basis of a channel estimate, and the second feedback signal may define a second phase weight
5 determined on the basis of a rotated constellation. In particular, the second phase weight may be based on a rotated channel estimate of the same constellation, or on a rotated channel estimate of another constellation, or on the basis of a quantization of the channel estimate to the
10 second (rotated) constellation. The first and second feedback signals may be fed back in successive time slots. Moreover, the first feedback signal may define a real part of the weight information, and the second feedback signal may define an imaginary part of the weight information.

15

Alternatively, the first feedback signal may define a first feedback information to be used for updating a first beam of the transmitting element, and the second feedback signal may define a second feedback information to be used for
20 updating a second beam of the transmitting element. In this case, the first feedback signal can be fed back during odd time slots and the second feedback signal during even time slots. The odd and even time slots may be used for controlling the same antenna (when the channel difference
25 is used) or a first antenna and a second antenna, respectively, in different time instants. In the latter case, the first and second antennas are alternately used as a reference. Controlling both antennas, e.g. by transmitting control commands in an alternate manner to the
30 transmitting element, is preferred in cases where the effective transmitting power of the controlled antenna can be reduced by the filtering. When both antennas are generally controlled, the effective transmitting power is distributed evenly and this simplifies the designs of a
35 provided power amplifier. Another possible solution is to

- 12 -

use transmit diversity techniques where different users may control different antennas.

Furthermore, the first feedback signal may define a
5 quadrant in a 4-PSK constellation, and the second feedback signal may define a constellation within said quadrant defined by said first feedback signal. The second feedback signal may define a differential change, a Gray-encoded sub-quadrant, or a combination thereof.

10 The multiplexed feedback signals may be transmitted by at least two users having different feedback signal constellations. Thereby, a flexible and readily adaptable transmit diversity system can be achieved. The at least two users may comprise a first set of users controlling weights
15 at a first antenna of the transmitting element, and a second set of users controlling weights at a second antenna of said transmitting element. In this case, a useful balancing of the transmitting power between the first and second antennas can be provided, since some filtering or
20 demultiplexing techniques may result in lower transmission power requirements at the controlled antenna.

Furthermore, the control means provided in the transmitter may comprise a switching means for alternately switching
25 the first feedback signal and the second feedback signal to the determining means. The determining means may be arranged to derive the weight information from the first and second feedback signal.

30 Moreover, the control means may be arranged to control the transmitting means so as to alternately update a first beam of the transmitting element by using a first weight information determined on the basis of the first feedback signal, and a second beam of the transmitting element by

- 13 -

using a second weight information determined on the basis of the second feedback signal.

The transmitting element may be an antenna array. In this case, the feedback information can be used for controlling the direction of transmission of the array antenna. The transmission direction may be derived from at least one of the multiplexed feedback signals. Furthermore, the transmission direction may be derived from a phase estimate obtained from at least one feedback signal.

Furthermore, the deriving means of the receiver may comprise extracting means for extracting a probing signal transmitted with a known power, channel estimation means for performing a channel estimation on the basis of the extracted probing signal, and generating means for generating the multiplexed feedback signals on the basis of the channel estimation. The generating means may be arranged to generate the first and second feedback signal, wherein the feedback means may be arranged to feed back the first and second feedback signals as the multiplexed feedback signals. The first and second feedback signals may be fed back alternately by the feedback means, wherein a quantization of the feedback information is based on the latest channel estimate and an available one of the first and second constellation.

Moreover, the generating means may be arranged to generate the first feedback signal based on the channel estimate and the second feedback signal based on a rotation of the channel estimate by a predetermined angle. This can be implemented also by quantizing the same channel estimate to two constellations where, in this case, the second one is a rotated copy of the first one.

- 14 -

Alternatively, the generating means may be arranged to generate the first feedback signal based on a real part of the feedback information, and the second feedback signal based on an imaginary part of the feedback information.

5

As a further alternative, extracting means may be arranged to alternately extract a probing signal corresponding to a first beam and a probing signal corresponding to a second beam, and the generating means may be arranged to

10 alternately generate the first feedback signal based on a channel estimate for the first beam, and the second feedback signal based on a channel estimate for the second beam.

15

BRIEF DESCRIPTION OF THE DRAWINGS

In the following, the present invention will be described in greater detail on the basis of a preferred embodiment with reference to the accompanying drawings, in which:

20

Fig. 1 shows a principle block diagram of a closed-loop transmit diversity system comprising a base station and a mobile station,

25 Fig. 2 shows a table indicating characteristic parameters of the FB modes 1 to 3,

Figs. 3A to 3C show tables indicating characteristic parameters relating to the feedback control of the FB modes

30 1, 2 and 3, respectively,

Fig. 4 shows tables indicating characteristic parameters of the transmit diversity concept according to a first example of the preferred embodiment of the present invention,

35

- 15 -

Fig. 5 shows a principle block diagram of a base station and a mobile station according to the preferred embodiment of the present invention,

5 Fig. 6 shows a diagram of complex weight parameters according to the first example of the preferred embodiment,

Fig. 7 shows tables indicating characteristic parameters of the transmit diversity concept according to a second
10 example of the preferred embodiment,

Fig. 8 shows a diagram of complex weight parameters according to the second example of the preferred embodiment.

15

DESCRIPTION OF THE PREFERRED EMBODIMENT

In the following, the preferred embodiment of the method and system according to the present invention will be
20 described on the basis of a connection between the BS 10 and the MS 20 of the UMTS, as shown in Fig. 1.

According to the preferred embodiment of the present invention, the feedback information is transmitted from the
25 MS 20 to the BS 10 using a feedback concept based on time multiplexing. This means that the constellation of the feedback signals is changed and signaled to the BS 10 in different time slots. However, any other multiplex scheme such as frequency multiplexing or code multiplexing may be
30 used as well in the feedback channel.

In particular, the feedback signal constellation may be changed with respect to the coding, type, partitioning or allocation of the feedback information. Thus, with the
35 present time multiplexed feedback subchannels, the

- 16 -

signaling capacity required in the feedback channel can be maintained, while the feedback information as such is spread over the time axes, i.e. transmitted in two or more (sets of) time slots which may be allocated according to a predefined rule, known to both the BS 10 and the MS 20.

In the following, three examples of the preferred embodiment are described with reference to Figs. 4 to 8, wherein the feedback information is spread over successive time slots.

Fig. 4 shows two tables indicating a refined mode 2 concept. According to this example, two reference channels, i.e. the channel estimate and a rotated channel estimate, are used in the MS 20 in order to derive the feedback information. Thereby, an 8-phase signaling can be implemented by using the mode 2 feedback signaling, i.e. two feedback bits. In particular, a first feedback information relating to the channel estimate is transmitted in two successive time slots, and a second feedback information relating to the rotated channel estimate is transmitted in the following two successive time slots. Thus, the whole feedback information is transmitted in four successive time slots. Accordingly, the phase difference relating to the channel estimate is transmitted in slots $S1 = \{1, 2, 5, 6, 9, 10, \dots\}$ defining a first feedback subchannel, and the phase difference quantized to the rotated constellation is transmitted in slots $S2 = \{3, 4, 7, 8, 11, 12, \dots\}$ defining a second feedback subchannel, wherein the rotated channel estimate relates to a 45° rotated channel estimate, assuming a 4-phase constellation is used.

Thus, the effective phase differences for the phase bits transmitted in the slots $S1$ is indicated by the upper table

- 17 -

of Fig. 4, and the phase difference defined by the phase bits transmitted in the slots S2 is indicated in the lower table of Fig. 4. Accordingly, the phase difference can be quantized into 8 values while using only two bits of
5 feedback information at a time, as in the FB mode 2. The resulting feedback resolution obtained by a filtering or demultiplexing operation at the BS 10 corresponds to the FB mode 3, with the exception that a constant power is used for each of the antennas A1 and A2. Thus, the feedback
10 resolution can be increased while maintaining the feedback signaling capacity of the FB mode 2.

Fig. 5 shows a principle block diagram of the MS 20 and the BS 10 according to the preferred embodiment of the present
15 invention.

According to the Fig. 5, the BS 10 comprises a transceiver (TRX) 11 arranged for feeding the two antennas A1 and A2 and connected to an extracting unit 12 provided for
20 extracting the feedback information transmitted from the MS 20 via the corresponding feedback channel(s). The extracted feedback information is supplied to a switch 13 which is controlled by a timing control unit 15 in accordance with the timing scheme underlying the multiplex scheme of the
25 feedback signal constellation used by the MS 20. Thereby, a demultiplexing or filtering function for extracting the feedback information is provided. In the present example, the switch 13 is controlled by the timing control unit 15 so as to supply the feedback information relating to the
30 slots S1 to one of its output terminals and the feedback information transmitted in the slots S2 to the other one of its output terminals.

It is noted that the above demultiplexing or filtering
35 function may alternatively be achieved by providing filter

- 18 -

and demodulating unit or a decoding unit, in case a frequency or, respectively, code multiplex scheme is used.

The output terminals of the switch 13 are connected to
5 respective input terminals of a weight determination unit 14 which determines a weight signal on the basis of the tables shown in Fig. 4. In particular, the weight determination unit 14 determines the required phase difference between the antennas A1 and A2 by averaging the
10 feedback information of the two slot types S1 and S2 received via the respective input terminals. However, any other combination of the two feedback informations may be provided.

15 The determined weight signal, e.g. phase difference, is supplied to the TRX 11 which performs a corresponding phase control of the antennas A1 and A2 to thereby establish the required phase difference leading to an optimum coherence of the transmission signals in the MS 20.

20 The MS 20 comprises a transceiver (TRX) 21 for receiving the transmission signals from the antennas A1 and A2 of the BS 10 via an antenna connected thereto. Furthermore, the TRX 21 is connected to an extracting unit 22 provided for
25 extracting the pilot channel signal and supplying the extracted pilot channel signal to a channel estimation unit 23 which calculates the required channel estimates. In particular, the channel estimation unit 23 is arranged to calculate the channel estimate and the rotated channel
30 estimate both corresponding to the received pilot channel signal. The channel estimation unit 23 outputs the two channel estimates at respective output terminals thereof which are connected to corresponding input terminals of a channel difference deriving and quantization unit 24 for
35 deriving a phase difference based on the channel estimate

- 19 -

and the rotated channel estimate obtained from the channel estimation unit 23 and performing a corresponding quantization. As already mentioned, the rotated channel estimate is obtained by rotating the channel estimate by an
5 angle of 45° .

Furthermore, a feedback timing unit 25 is provided which controls the phase difference deriving and quantization unit 24 so as to output one of the phase differences
10 derived from the channel estimate and the rotated channel estimate in accordance with the predetermined feedback timing. In the present case, the phase difference corresponding to the channel estimate, i.e. conventional FB mode 2, is outputted during the time slots S1, and the
15 phase difference corresponding to the rotated channel estimate is outputted during the time slots S2. The phase differences are supplied as a multiplexed feedback signal to the TRX 21 in order to be transmitted via the corresponding feedback channel to the BS 10.

20

It is to be noted that the transmit diversity concept according to the first example of the preferred embodiment is compatible with the known FB mode 2, in case the BS 10 assumes each feedback information as derived only from the
25 channel estimate which has not been rotated, i.e. the known BS 10 controlled according to the FB mode 2.

In case a frequency or code multiplex feedback scheme is used, the feedback timing unit 25 may be replaced by a
30 modulating unit or, respectively, a coding unit.

Fig. 6 shows a diagram of the complex weights or end points of the weight vectors used as the feedback information in the first example of the preferred embodiment. In
35 particular, the circles in the diagram of Fig. 6 indicate

- 20 -

the weights obtained in the slots S1, i.e. the weight of the conventional FB mode 2, and the crosses indicate the additional weights obtained in the time slots S2. Thus, a phase difference quantization as provided in the FB mode 3
5 can be obtained without increasing the feedback channel signaling capacity.

Fig. 7 shows a second example of the preferred embodiment, wherein the feedback resolution of the FB mode 2 is
10 obtained while using only a single feedback bit. Thus, this example relates to a refined FB mode 1. In particular, the MS 20 performs a continuous measurement or channel estimation, e.g. on the basis of a sliding window, and the phase difference deriving unit 24 quantizes the phase
15 difference in accordance with the FB mode 2 phase constellation. In the present case, the feedback bits for the real and imaginary part of the complex weight, determined by the phase difference, are transmitted in successive slots, e.g. the real part bit in the odd slots
20 used as a first feedback subchannel and the imaginary part bit in the even slots used as a second subchannel. A corresponding control is performed by the feedback timing unit 25 of the MS 20.

25 Correspondingly, the timing control unit 15 of the BS 10 controls the switch 13 so as to supply the successive real and imaginary part of the feedback information to respective input terminals of the weight determination unit 14 which determines the corresponding weight signal
30 supplied to the TRX 11 in order to establish the required phase difference.

In case the BS 10 is not controlled in accordance with this time control scheme, i.e. the current FB mode 1 is used,
35 the conventional control is obtained. If the new timing

- 21 -

control is provided, the weight determination unit 14 averages over two slots and changes the weight signal correspondingly.

5 Thus, an FB mode 2 resolution is obtained with an FB mode 1 feedback capacity. Moreover, an antenna verification can be incorporated separately for the successive bits, which corresponds to the STD concept.

10 Thus, as can be gathered from Fig. 7, the feedback information provided in the odd slots S_{odd} indicates a phase difference of 0° or 180° , and the feedback information provided in the even slots S_{even} indicates a phase difference of -90° or $+90^\circ$.

15

Fig. 8 shows a diagram of the complex weights which can be fed back in the second example of the preferred embodiment, wherein the crosses indicate the weight information transmitted in the slots S_{even} and the circles indicate the weights transmitted in the slots S_{odd} .

20

According to a third example of the preferred embodiment, a beam diversity concept can be adopted by the feedback scheme in order to provide an enhanced robustness against erroneous signaling. In the third example, it is assumed that a space time coding (STTD) is used at the MS 20, wherein encoded channel symbols are divided into two-element blocks and transmitted as $b[2n]$, $b[2n+1]$ and $-b^*[2n+1]$, $b^*[2n]$ from the antennas A1 and A2, respectively, during time instants $2n$ and $2n+1$ using the same spreading code. This simple symbol level orthogonal coding scheme doubles the time diversity, wherein the receiver uses a simple linear decoding to detect the transmitted symbols. In the present case, two weight vectors are used, which are a function of the received signaling. In case of the FB

35

- 22 -

mode 1 feedback signaling, the following processing is performed.

Two beams B1 and B2 are transmitted by the antennas A1 and A2 of the BS 10 in each time slot. The update rate of the beams B1 and B2 is 800 Hz, i.e. the TRX 11 is updated every other time slot. In particular, the beam B1 is modified during odd slots and the beam B2 during even slots, where each weight modification is effective over two time slots, i.e. a sliding window weight change is provided. Hence, the extracting unit 22 of the MS 20 is arranged to extract the corresponding probing or pilot signals received from the the beams B1 and B2, and to successively supply them to the channel estimation unit 23. Then, the feedback timing unit 25 controls the phase difference deriving unit 24 so as to output the respective phase differences at timings corresponding to their allocated time slots.

It is to be noted that the filtering function provided by the switch unit 13 and the timing control unit 15 of the BS 10 is not required in the present case, if the TRX 11 is arranged to determine and correspondingly allocate successively received weight signals to their respective beams B1 or B2. However, if this is not the case, the timing control unit 15 controls the switch 13 so as to switch the weight signal of the beam B1 (transmitted in an odd slot) to one of its output terminals and the weight signal of the beam B2 (transmitted in an even slot) to the other output terminal and the weight determination unit 14 determines the corresponding weight signal. In addition, the timing control unit 15 is arranged to control the TRX 11 so as to allocate the received weight signal to the corresponding one of the beams B1 and B2. This control feature is indicated by the broken error shown in the block diagram of the BS 10 of Fig. 5.

- 23 -

It is to be noted that the above described units of the block diagram shown in Fig. 5 may as well be established as software features of a control program controlling a microprocessor such as a CPU provided in the BS 10 and the MS 20.

Furthermore, any kind of signal set partitioning (e.g. for trellis codes) may be used to improve the performance.

Furthermore, the different feedback signal constellations may be dependent by using a progressive signaling. For example, a first time slot or subchannel can be used for feeding back an information indicating a quadrant in a 4-PSK constellation with higher reliability, and a subsequent second time slot or subchannel can be used for feeding back an information determining the constellation within this quadrant. The feedback information of the second subchannel may be based on a differential change, a Gray-encoded sub-quadrant, or any combination thereof. Here, the transmit weights can be changed as soon as the feedback bits specifying the quadrant have arrived at the BS 10, and the refined subquadrant can be adjusted thereafter based on the most recent channel estimate, which was not available when the quadrant index was transmitted (e.g. using Gray encoding). Thereby, additional delay caused in the current concept by waiting for the receipt of all feedback bits can be prevented. Furthermore, abrupt changes (180 degree in case of one bit feedback, 90 degrees in case of two bit feedback, and so on), as in the current concepts, which cannot be followed by the MS 20 estimating the dedicated channel parameters do not occur. Hence, applying the feedback information incrementally not only reduces delay, but also enables more efficient channel estimation and receiver performance. The feedback information may also refer to the phase difference of successive slots.

- 24 -

Furthermore, the present invention is not limited to two antennas A1 and A2, but can be applied to any multi-antenna transmitter in order to provide a higher resolution

5 feedback. Moreover, as already mentioned, any kind of multiplex scheme can be used, provided the BS 10 is arranged to correspondingly filter or select the feedback information.

10 Furthermore, the present invention may be applied to any wireless communication system comprising a transmit diversity or transmit beamforming concept used between a transmitting element and at least one receiver. Therefore, the above description of the preferred embodiment and the
15 accompanying drawings are only intended to illustrate the present invention. The preferred embodiment of the invention may vary within the scope of the attached claims.

In summary, the invention relates to a transmit diversity
20 method for a wireless communication system comprising a transmitting element and at least one receiver, wherein a transmission signal is transmitted from the transmitting element to the at least one receiver in accordance with a weight information determined in response to a feedback
25 information. The feedback information is derived from the response at the at least one receiver to the transmission signal, and is fed back using multiplexed feedback signals. Thus, multiple quantization constellations and/or constellation specific feedback subchannels can be used for
30 channel probing, such that the total feedback resolution can be enhanced, while maintaining low signaling capacity of the feedback channel.

- 25 -

Claims

1. A transmit diversity method for a wireless communication system comprising a transmitting element and
5 at least one receiver, said method comprising the steps of:
a) transmitting from said transmitting element to said at least one receiver a transmission signal in accordance with a weight information determined in response to a feedback information;
10 b) deriving said feedback information from the response at said at least one receiver to said transmission signal;
c) feeding back said feedback information using multiplexed feedback signals.
- 15 2. A method according to claim 1, wherein said multiplexed feedback signals comprises a first feedback signal having a first quantization constellation and a second feedback signal having a second quantization constellation.
- 20 3. A method according to claim 2, wherein said first and second feedback signals are transmitted in different time slots.
- 25 4. A method according to claim 2 or 3, wherein said first and second feedback signals are transmitted using different codes.
5. A method according to anyone of claims 2 to 4, wherein
30 said first feedback signal defines a first weight determined on the basis of a channel estimate quantized to said first constellation, and said second feedback signal defines a second weight determined on the basis of a channel estimate quantized to said second constellation.

35

- 26 -

6. A method according to claim 5, wherein said second constellation is a rotated copy of said first constellation.

5 7. A method according to claim 5, wherein said second feedback signal is based on a rotated channel estimate quantized to said first constellation.

8. A method according to claims 2 or 3, wherein said
10 first and second feedback signals are fed back in successive time slots.

9. A method according to anyone of claims 2, 3 or 8,
wherein said first feedback signal defines a real part of
15 said weight information, and said second feedback signal defines an imaginary part of said weight information.

10. A method according to anyone of claims 2, 3 or 8,
wherein said first feedback signal defines a first feedback
20 information to be used for updating a first beam of said transmitting element, and said second feedback signal defines a second feedback information to be used for updating a second beam of said transmitting element.

25 11. A method according to claim 9 or 10, wherein said first feedback signal is fed back during odd time slots, and said second feedback signal is fed back during even time slots.

30 12. A method according to anyone of claims 2, 3 or 8, wherein said first feedback signal defines a quadrant in a 4-PSK constellation, and said second feedback signal defines a constellation point within said quadrant defined by said first feedback signal.

- 27 -

13. A method according to claim 12, wherein said second feedback signal defines a differential change, a Gray-encoded sub-quadrant, or a combination thereof.

5 14. A method according to claim 1, wherein said multiplexed feedback signals are transmitted by at least two users having different signal constellations.

10 15. A method according to claim 14, wherein said at least two users comprise a first set of users controlling weights at a first antenna of said transmitting element, and a second set of users controlling weights at a second antenna of said transmitting element.

15 16. A method according to claim 1, wherein said feedback information is used for controlling a transmit weight of one of two antennas.

20 17. A method according to claim 1, wherein said feedback information is used for controlling transmit weights of two antennas.

25 18. A method according to claim 17, wherein control commands for controlling said two antennas are transmitted alternately to said transmitting element.

19. A method according to claim 1, wherein said transmitting element comprises an antenna array.

30 20. A method according to claim 19, wherein said feedback information is used for controlling the direction of transmission of said antenna array.

- 28 -

21. A method according to claim 20, wherein the direction of transmission is derived from at least one feedback signal.

5 22. A method according to claim 21, wherein the direction of transmission is derived from a phase estimate of at least one extracted feedback signal.

10 23. A method according to claim 1, wherein said weight information and/or a direction of transmission are determined on the basis of a feedback signal filtering operation.

15 24. A method according to claim 23, wherein said filtering operation comprises a robust filtering, an FIR filtering, an IIR filtering, a linear filtering, a non-linear filtering, or a smoothing and prediction.

20 25. A method according to anyone of the preceding claims, wherein a reliability of said multiplexed feedback signals is used for weight determination.

25 26. A method according to claim 23 or 24, wherein a transmission filtering is adapted to a transmission channel characteristic and changed dynamically.

27. A transmit diversity system for a wireless communication system, comprising:

- a) transmitting means (10) for transmitting a
30 transmission signal from a transmitting element (A1, A2) in accordance to with a weight information determined in response to a feedback information; and
- b) at least one receiver (20) for receiving said transmission signal and deriving said feedback information
35 from the response to said transmission signal;

- 29 -

c) wherein said at least one receiver (20) comprises feedback means (24, 25) for feeding back said feedback information using multiplexed feedback signals.

5 28. A system according to claim 27, wherein said feedback means (24, 25) is arranged to generate a first feedback signal having a first constellation and a second feedback signal having a second constellation.

10 29. A system according to claim 28, wherein said first feedback signal defines a first phase weight determined on the basis of a channel estimate, and said second feedback signal defines a second phase weight determined on the basis of a rotated constellation of said first feedback
15 signal.

30. A system according to claim 28, wherein said first feedback signal defines a real part of said weight information, and said second feedback signal defines an
20 imaginary part of said weight information.

31. A system according to claim 28, wherein said first feedback signal defines a first feedback information to be used by said transmitting means (10) for updating a first
25 beam of said transmitting element (A1, A2), and said second feedback signal defines a second feedback information to be used by said transmitting means (10) for updating a second beam of said transmitting element (A1, A2).

30 32. A system according to claim 30 or 31, wherein said feedback means (24, 25) is arranged to feed back said first feedback signal during odd time slots and said second feedback signal during even time slots.

- 30 -

33. A transmitter for a wireless communication system, comprising:

- a) extracting means (12) for extracting a feedback information from a received signal;
- 5 b) transmitting means (11) for transmitting a transmission signal from a transmitting element (A1, A2) in accordance with a weight information;
- c) determining means (14) for determining said weight information in response to said extracted feedback
- 10 information; and
- d) control means (13, 15) for controlling said determining means (14) so as to determine said weight information in accordance with multiplexed feedback signals used for feeding back said feedback information.

15

34. A transmitter according to claim 33, wherein said control means (13, 15) comprises a switching means (13) for alternately switching a first feedback signal having a first constellation and a second feedback signal having a

20 second constellation to said determining means (14).

25

35. A transmitter according to claim 34, wherein said determining means (14) is arranged to derive said weight information from said first and second feedback signals.

30

36. A transmitter according to claim 34, wherein said control means (13, 15) is arranged to control said transmitting means (11) so as to alternately update a first beam of said transmitting element (A1, A2) by using a first

weight information determined on the basis of said first feedback signal, and a second beam of said transmitting element (A1, A2) by using a second weight information determined on the basis of said second feedback signal.

- 31 -

37. A transmitter according to anyone of claims 33 to 36, wherein said transmitting element is an antenna array (A1, A2).

5 38. A receiver for a wireless communication system, comprising:

a) receiving means (21) for receiving a transmission signal;

b) deriving means (22, 23, 24) for deriving a feedback
10 information from the response to said transmission signal;
and

c) feedback means (24, 25) for feeding back said feedback information using multiplexed feedback signals.

15 39. A receiver according to claim 38, wherein said deriving means (22, 23, 24) comprises extracting means (22) for extracting a probing signal transmitted with a known power, channel estimation means (23) for performing a channel estimation on the basis of said extracted probing
20 signal, and generating means (24) for generating said multiplexed feedback signals on the basis of said channel estimation.

40. A receiver according to claim 39, wherein said
25 generating means (24) is arranged to generate a first feedback signal having a first constellation and a second feedback signal having a second constellation, wherein said feedback means (24, 25) is arranged to feed back said first and second feedback signals as said multiplexed feedback
30 signals.

41. A receiver according to claim 40, wherein said feedback means (24, 25) is arranged to alternately feed back said first and second feedback signals, wherein a
35 quantization of the feedback information is based on the

- 32 -

latest channel estimate and an available one of said first and second constellation.

42. A receiver according to claim 40, wherein said
5 generating means (24) is arranged to generate said first feedback signal based on said channel estimation and said second feedback signal based on a rotation of said channel estimation by a predetermined angle.

10 43. A receiver according into claim 40, wherein said generating means (24) is arranged to generate said first feedback signal based on a real part of said feedback information, and said second feedback signal based on an imaginary part of said feedback information.

15 44. A receiver according to claim 40, wherein said extracting means (22) is arranged to alternately extract a probing signal corresponding to a first beam and a probing signal corresponding to a second beam, and said generating
20 means (24) is arranged to alternately generate said first feedback signal based on a channel estimate for said first beam, and said second feedback signal based on a channel estimate for said second beam.

25

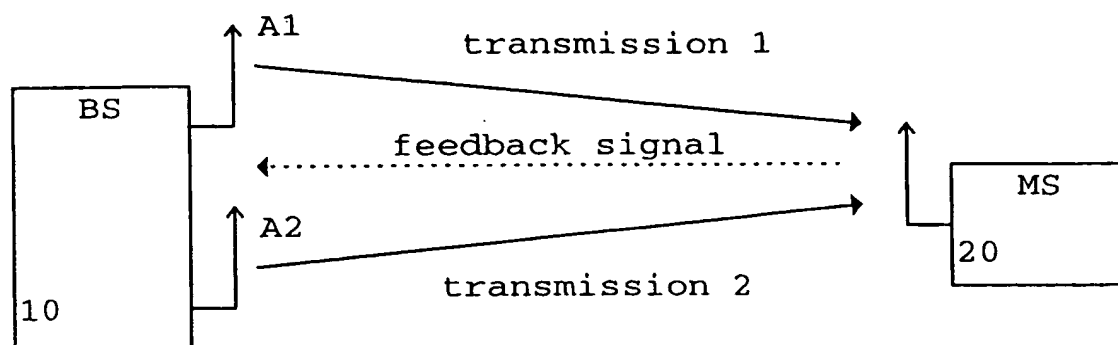


Fig. 1

FB mode	N_{FB}	N_W	update rate	feedback bit rate	N_a	N_p
1	1	1	1600/s	1600bps	1	0
2	1	2	800/s	1600bps	0	2
3	1	4	400/s	1600bps	1	3

Fig. 2

feedback value	P_{A1}	P_{A2}
0	0	1
1	1	0

Fig. 3A

feedback value	phase - diff.
0 0	180°
0 1	-90°
1 1	0°
1 0	90°

Fig. 3B

ampl. bit	P _{A1}	P _{A2}
0	0.2	0.8
1	0.8	0.2

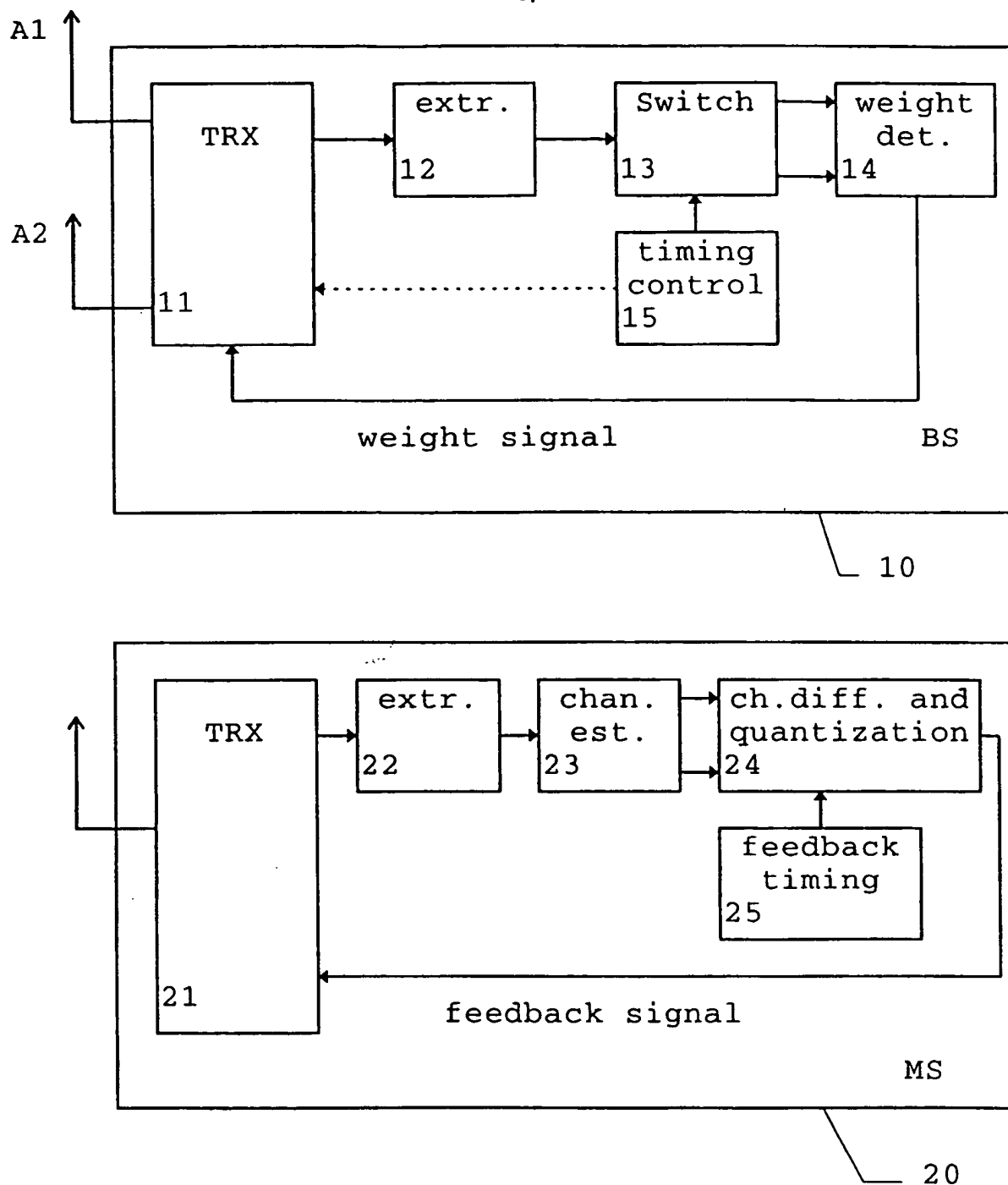
phase bits	phase diff.
0 0 0	180°
0 0 1	-135°
0 1 1	-90°
0 1 0	-45°
1 1 0	0°
1 1 1	45°
1 0 1	90°
1 0 0	135°

Fig. 3C

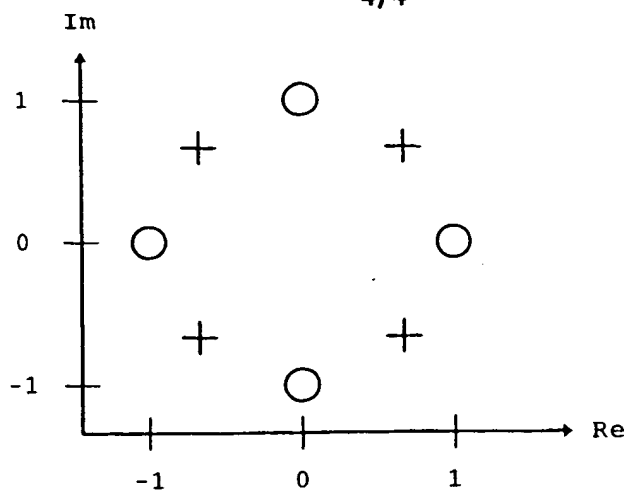
phase bits (slots S1)	phase difference
0 0	180°
0 1	-90°
1 1	0°
1 0	90°

phase bits (slots S2)	phase difference
0 0	-135°
0 1	-45°
1 1	45°
1 0	135°

Fig. 4

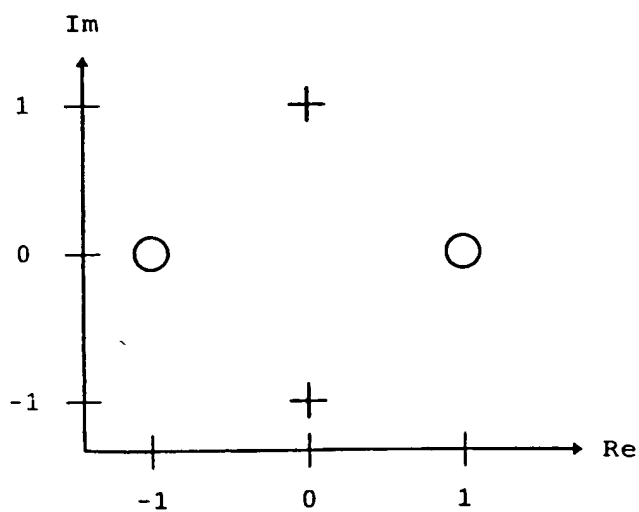
**Fig. 5**

4/4

**Fig. 6**

phase bit (S_{odd})	phase difference
0	180°
1	0°

phase bit (S_{even})	phase difference
0	-90°
1	$+90^\circ$

Fig. 7**Fig. 8**